

Data-compensating power measurement

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BACKGROUND OF THE INVENTION

1. Technical Field

10 The present invention relates to power measurements for linearly modulated radio frequency signals and more particularly to a method and a device for compensating a data-dependency of a power measurement caused by linear modulation.

2. Discussion of the Prior Art

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20 The condition of radio systems such as mobile phone systems or satellite systems has to be constantly monitored by power measurements to ensure a high quality of transmission and to avoid damages occurring at output stages that resulting from excessively high power levels.

25 Within current transceiver units in the Global System for Mobile Communications (GSM) base transceiver stations a measurement of the output power (P_{fwd}) transmitted via an output port and a separate measurement of the power, which is reflected (P_{refl}) at the output port, are performed. P_{fwd} is e.g. measured at the beginning of the useful part of a transmitted Gaussian Minim Shift Keying (GMSK) burst and P_{refl} is e.g. measured at the end of the useful part of the burst. The power measurements are thus performed time multiplexed.

35 Based on the measured values of P_{fwd} and P_{refl} , the condition of the base transceiver station can be assessed, e.g. by calculating the voltage standing wave ratio (VSWR). In WO94/24576 a method for supervising the condition of a transmitter antenna of

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a radio system based on the VSWR is described. The VSWR is a measurement of impedance mismatch between a transmission line and its load. The higher the ratio, the greater the mismatch. In other words, as the VSWR increases, the transmission quality declines.

The GMSK modulation technique is a non-linear modulation technique which introduces only very small variations of the radio frequency signal envelope during the useful part of the burst.

10 The powers P_{fwd} and P_{refl} are not data dependent and thus can be measured at arbitrary instances in time during a burst. The measurement results can be used directly for the calculation of the matching VSWR.

15 Linear modulation techniques insert large variations in output power depending on the sequence of data which are transmitted. The dynamic power range spreads up to 19dB over the useful part of the burst, as shown in Fig. 5. The measurement of P_{fwd} and P_{refl} during the useful part of the burst does not lead to reliable results for linear modulation technique, due to the data dependency of the output power. The maximum variation in average output power due to linear modulation between the first and the second half of a single burst can attain 2dB if every symbol is measured and used for calculating the average output power. If

20 less symbols are measured, the maximum variation in average output power might even increase.

These data-dependent fluctuations of the average output power within a single burst may lead to serious problems when assessing the condition of a radio system based on time-multiplexed measurements. If, e.g., the real VSWR and the calculated VSWR differ by 2dB or more due to the data-dependency of the output power, the system may e.g. conclude that an antenna feeder cable is disconnected and an alarm will erroneously be sent. The inaccuracy of power measurements resulting from the data-dependency

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of the output power can thus lead to misinterpretations of the result of the VSWR calculation. Even more severe problems can result from misinterpretations of measurements of P_{fwd} since the measured value of P_{fwd} is an important parameter for the correct
5 supervision of the output power in order to avoid damages resulting from excessively high output power levels.

There is, therefore, a need for a method and device for compensating the data-dependency of time multiplexed measurements of
10 P_{fwd} and P_{refl} for linear modulation techniques.

SUMMARY OF THE INVENTION

15 The present invention satisfies this need by providing a method for compensating a data-dependency of a power measurement caused by linear modulation, comprising performing a first measurement of a transmitted output power, performing a second measurement of a reflected power, wherein the second measurement
20 is performed time multiplexed from said first measurement, calculating a first average power based on data transmitted during the first measurement, calculating a second average power based on data transmitted during the second measurement, and compensating at least one of the first measurement and second measurement
25 based on a difference between the first average power and the second average power.

A device according to the invention for compensating a data-dependency of a power measurement caused by linear modulation
30 comprises a modulator for linearly modulating a data signal, a measurement unit for performing a first measurement of a transmitted output power and a second measurement of a reflected power, wherein the second measurement is performed time multiplexed from said first measurement, and a compensating unit for
35 compensating at least one of the first measurement and second

measurement based on a difference between a first average power and a second average power. The device further comprises at least one of a calculating unit for calculating the first average power based on data transmitted during the first measurement
5 and the second average power based on data transmitted during the second measurement and a database for storing a difference between the first average power the second average power.

The invention allows to perform power measurements within arbitrary time windows and independent of the structure of a particular burst. The first and second measurements may be performed prior to, concurrently with or after calculating the first and second output powers depending on whether or not the transmitted data are known prior to the first and second measurements.
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15 Preferably, the first and second measurements are integrating measurements or are performed by means of averaging a plurality of single measurements.

According to the invention, the first and second measurements are performed time multiplexed, i.e., during different time windows. Since the first and second measurements are performed time multiplexed, the hardware cost can be reduced because both measurements are preferably performed by e.g. a single measurement ASIC. The invention thus allows the adaptation of conventional
20 power measurement methods and devices which were hitherto used for non-linearly modulated signals to linear modulation techniques like 8-PSK signals.
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In GSM, a burst, i.e., a transmission quantum, consists of a plurality of data sequences. The plurality of data sequences comprises a first tail bit sequence, a first user data sequence, a training sequence, a second user data sequence, and a second tail bit sequence. The first measurement and the second measurement can be performed in the user data sequences, in the training sequence or in the tail bit sequences of a burst. Moreover,
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the first and the second measurement can be performed both in a single burst or in different bursts.

If the first measurement and the second measurement are per-
5 formed in different bursts, at least one of the measurements is preferably also compensated based on a difference in the configured power level of the different bursts. This takes into account that the output power might not only vary from one burst to another due to the data-dependency of the signal envelope,
10 but also due to changes in the configured power level. If, e.g., the transmission conditions improve from one burst to another, the system may automatically reduce the maximum output power level.

15 It was pointed out above that the first measurement and the second measurement may be performed in the user data sequences, in the training sequences or in the tail bit sequences. According to a first embodiment of the invention, the first and the second measurements are performed in different types of data sequences.
20 Therefore, the first measurement may e.g. be performed in a user data sequence and the second measurement may be performed in a tail bit sequence. Other permutations are likewise possible.

According to a second embodiment of the invention, the first
25 measurement and the second measurement are performed within the same type of data sequences. Thus, both the first and the second measurements may e. g. be performed within a single or within different user data sequences and the first average power and the second average power may be calculated based on the user
30 data comprised within the user data sequence or user data sequences. However, the first measurement and the second measurement can also both be performed within a single or, if the configured power levels of the two bursts are known, within different training sequences. The first average power and the second
35 average power can then be calculated based on the training se-

quence data. Since training sequences comprise standardized data that are known prior to the measurements, the difference between the first average power and the second average power may be calculated prior to the measurements and be stored in a database.

5 Also, the first measurement and the second measurement can both be performed within a single or within different tail bit sequences. If the measurements are performed within different tail bit sequences, the different tail bit sequences can be part of a single burst or of different bursts. The first and the second
10 average power can then be calculated based on the tail bit data.

Preferably, both the first and the second measurements are performed before an output port of e.g. a transceiver unit or a combining and distribution unit. A further component may be connected to the respective output port. This allows to determine
15 the matching of the further component based on a compensated measurement. In order to determine the matching, the VSWR may be calculated. The provision of calculating means for calculating the VSWR is therefore advantageous. The measurements are preferably performed in accordance with specific timing events.
20 Thus, a database for storing the timing events can be provided.

According to the invention, the above method for compensating a data-dependency of a power measurement can also be used for
25 monitoring the condition of a transmitting and receiving path within a transceiver unit. Thus, both the first and the second measurements can be performed within the transceiver unit and preferably between a radio frequency mixer and a power amplifier of the transceiver unit. The data between the radio frequency
30 mixer and the power amplifier can be routed on the board of the transceiver unit to the receiver. The receiver may then detect the routed data, determine a power level and calculate a bit error rate. The power level can be determined in accordance with the above illustrated method.

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BRIEF DESCRIPTION OF THE DRAWINGS

Further aspects and advantages of the invention will become apparent upon reading the following detailed description of preferred embodiments of the invention and upon reference to the drawings in which:

- FIG 1. shows a block diagram of device for compensating a data-dependency of a power measurement caused by linear modulation according to the invention;
- FIG 2. shows a first graph of a GSM burst;
- FIG 3. shows a second graph of a GSM burst;
- FIG 4. shows a graph of the power level differences;
- FIG 5. shows a graph of a linear modulation burst; and
- FIG 6. shows a block diagram of a double measurement receiver.

DESCRIPTION OF PREFERRED EMBODIMENTS

Referring now to the accompanying drawings, the preferred embodiments of this invention are described.

In Fig. 1, a schematic diagram of several components of a device for compensating a data-dependency of a power measurement caused by linear modulation within a base transceiver station 100 is illustrated. The base transceiver station 100 is part of a cellular communication system and comprises a transceiver unit 120 in communication with a combining and distribution unit 110, and an antenna 101 in communication with the combining and distribution unit 110.

The measurement receiver 160 may also be located within the combining and distribution unit 120, whereby the transmitted output power P_{fwd} and the reflected power P_{refl} are transmitted to the transceiver unit 120 via a digital bus. If the measurement receiver 160 is located within the combining and distribution unit 120, the digital bus may also be used for transferring a VSWR calculated in the combining and distribution unit 110 to the transceiver unit 120.

The measurement receiver 160 detects the power levels of the transmitted output power P_{fwd} and the reflected power P_{refl} . P_{fwd} and P_{refl} can be measured in separate parts of a burst or in different bursts, with knowledge of the configured power level in the current burst. The measured power levels $P_{\text{fwd, meas}}$ and $P_{\text{refl, meas}}$ are then converted into a digital signal by the analog/digital converter 161 and transmitted to a radio control firmware 171 in the radio controller 170.

As will be described below, the radio control firmware 171 may serve both as a calculating unit for calculating a first average power based on data transmitted during the first measurement and a second average power based on data transmitted during the second measurement and as a calculating unit for calculating the VSWR based on the previously calculated first and second average powers. Moreover, the radio control firmware 171 may be used as a compensating unit for compensating at least one of the first measurement and the second measurement based on a difference between the calculated first and second average power.

The radio control firmware 171 may receive data input from the baseband-filtered in-phase (I_{ik}) and quadrature-phase (Q_{ik}) data bits, the measured power levels $P_{\text{fwd, meas}}$ and $P_{\text{refl, meas}}$, and timing events from a database stored in the E-prom 162, and may calculate the VSWR as described below in more detail. The baseband-filtered in-phase (I_{ik}) and quadrature-phase (Q_{ik}) data bits are obtained from the corresponding "hard" bits I' and Q' by burst-shaping in a burst-shaping unit 130 and by interpolation in two parallel interpolaters 140 within the radio controller 170. The timing events stored in the database of the E-prom 162 assign the radio control firmware 171 exact timing points for the measurement of the transmitted output power P_{fwd} and the reflected power P_{refl} .

In the following, the method according to the invention for compensating a data-dependency of a power measurement caused by linear modulation within the base transceiver station 100 is described in more detail. As an example, monitoring the condition of the base transceiver station 100 by means of the VSWR is illustrated.

Figs. 2 and 3 show two exemplary embodiments according to the invention for measuring P_{fwd} and P_{refl} within a single burst 200 in GSM. In GSM, a burst consists of two tail bit sequences 210, 220, one after power ramping up and the other before power ramping down, a training sequence 230 arranged between the two tail bit sequences 210, 220, and two user data sequences 240, 250. A first user data sequence 240 is arranged between the first tail bit sequence 210 and the training sequence 230 and a second user data sequence 250 is arranged between the training sequence 230 and the second tail bit sequence 220.

According to the measurements depicted in Fig. 2, P_{fwd} and P_{refl} are measured time-multiplexed within the different user data sequences 240, 250. P_{fwd} is measured during a first time window within the first user data sequence 240 and P_{refl} is measured during a second time window within the second user data sequence 250.

Alternatively, P_{fwd} and P_{refl} may be measured during separate time windows within the training sequence 230 as depicted in Fig. 3. The training sequence 230 gives the advantage of putting less stringent requirements on the dynamic range of the measurement receiver 160 because of relatively small power variations of typically 4.5 dB compared to 19 dB during the user data sequences 240, 250 of the burst 200.

In the embodiments depicted in Figs. 2 and 3, the measurement of P_{fwd} is performed prior to the measurement of P_{refl} . Of course,

the measurement of P_{fwd} can also be performed after the measurement of P_{refl} .

Besides measuring current values of P_{fwd} and P_{refl} , the average powers during the respective time windows of the measurements of P_{fwd} and P_{refl} have to be determined in order to compensate the data-dependency of P_{fwd} and P_{refl} . Generally, the measurement time windows need not to be identical with the averaging time windows.

The average powers can be calculated based on the I and Q data signals. Preferably, the values of the I and Q data after baseband data filtering are used. The arithmetical average of the powers may be calculated by means of different averaging algorithms. One possible averaging algorithm is:

$$P_{\text{out,calci}} = 10 \log_{10} \left[\frac{1}{N * L} * \sum_{i=1}^L \left(\sum_{k=1}^N (I_{ki}^2 + Q_{ki}^2) \right) \right]$$

where L is the length of the measured data sequence, i.e., the number of symbols. N is the amount of I and Q data samples after baseband data filtering and calci indicates the average power for the different measurement periods of P_{fwd} and P_{refl} . Thus, $P_{\text{out,calc1}}$ is the average power corresponding to the measurement of P_{fwd} and $P_{\text{out,calc2}}$ is the average power corresponding to the measurement of P_{refl} .

The difference $\Delta P_{\text{out,calc}}$ in average power during both measurements is then determined by subtracting the average power $P_{\text{out,calc2}}$ from the average power $P_{\text{out,calc1}}$. A representation of the difference $\Delta P_{\text{out,calc}}$ is shown in Fig. 4.

$P_{\text{out,calc1}}$ and $P_{\text{out,calc2}}$ may be calculated prior to, concurrently with or after the measurement of P_{fwd} and P_{refl} . If $P_{\text{out,calc1}}$ and

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$P_{out,calc2}$ are calculated concurrently with or after the measurement of P_{fwd} and P_{refl} , the I and Q data bits are received by the radio control firmware 171 on-line as they are output from the radio controller 170, and the radio control firmware 171 calculates $P_{out,calc1}$, $P_{out,calc2}$, and $\Delta P_{out,calc}$ on-line. This on-line calculation can be performed for the measurements depicted in Fig. 2 as well as for the measurements depicted in Fig. 3. In case of on-line calculations, the E-prom 162 depicted in Fig. 1 can be omitted.

The measurements depicted in Fig. 3 allow to calculate $P_{out,calc1}$, $P_{out,calc2}$ and $\Delta P_{out,calc}$ prior to the measurement of P_{fwd} and P_{refl} . This is due to the fact that the bit patterns of training sequences, and thus the I and Q data of the training sequences, are standardized and therefore known prior to the production of the TRU 120. In the standard GSM 05.02, e.g., eight different training sequence bit patterns for normal bursts modulated by 8-PSK are defined. The difference $\Delta P_{out,calc}$ can thus be calculated for these bit patterns and stored in a further database in the E-prom 162 during production of the transceiver unit 120. Together with $\Delta P_{out,calc}$, corresponding timing events for the radio control firmware 171 may be stored in a database in the E-prom 162. By means of the timing events it is ensured that P_{fwd} and P_{refl} are measured exactly during the time windows for which the stored value of $\Delta P_{out,calc}$ was calculated.

After P_{fwd} and P_{refl} have been measured, and after $\Delta P_{out,calc}$ has been calculated, the power levels used for calculating the VSWR can be determined by:

$$P_{fwd} = P_{fwd,meas}$$

$$P_{refl} = P_{refl,meas} + \Delta P_{out,calc}$$

Referring to the above equations and Fig. 4, it can be seen that the levels of $P_{out,calc1}$ and $P_{out,calc2}$ differ by $\Delta P_{out,calc}$. If P_{fwd} and P_{refl} have been measured in different bursts, the above equation of P_{refl} has to be corrected by an additive term which takes into account any difference between the configured power levels between the two bursts.

If the $P_{refl,meas}$ is measured between T3 and T4, it is smaller by $\Delta P_{out,calc}$, compared to a measurement between T1 and T2. Consequently, in the exemplary embodiment depicted in Fig. 4, $P_{refl,meas}$ is increased by adding the calculated difference $\Delta P_{out,calc}$.

In reality the calculated power levels are not the same as the measured power levels at the combining and distribution unit 110 output port 150 and the calculated powers will be distorted by an amplification factor a . Therefore, the above equations for P_{refl} and P_{fwd} have to be modified by

$$P_{fwd} = P_{fwd,meas} + 10 * \log_{10}(a)$$

$$P_{refl} = P_{refl,meas} + 10 * \log_{10}(a) + \Delta P_{out,calc}$$

Then, the square of the reflection coefficient r is calculated by

$$|r|^2 = \frac{P_{refl}}{P_{fwd}}$$

The VSWR, which is calculated in the radio controller 170, is given by

$$VSWR = \frac{1 + |r|}{1 - |r|}$$

As already pointed out, the VSWR is a measurement of impedance mismatch between the transmission line and its load. This measurement may be performed before the output port 153 of the combining and distribution unit 110, at an antenna connector itself or at an output port of the transceiver 110. The higher the VSWR, the greater the mismatch. In other words, as the voltage standing wave ratio increases and exceeds a predetermined value, an alarm is triggered signaling, for example, that the antenna 101 of the base transceiver station 100 has been disconnected.

Fig. 6 shows a further embodiment of a measurement receiver 400 for calculating the VSWR according to the invention in a linear modulation system. Contrary to the measurement receiver 160 depicted in Fig. 1, the double measurement receiver 400 comprises two measurement ASICs 410, 420 in parallel within the double measurement receiver 400. One ASIC 410 performs the P_{fwd} measurement and the other ASIC 420 a time-multiplexed P_{refl} measurement. The double measurement receiver 400 has to be supplied with by a signal splitter 450 with two synthesizer signals 430, 440 for converting the P_{fwd} and P_{refl} signals down.

In the above embodiments, P_{fwd} and P_{refl} have been measured either in a user data sequence or a training sequence. However, although the data-dependency of the signal envelope of the tail bit sequences is small, P_{fwd} and P_{refl} may also be measured in a tail bit sequence.